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CFAR Detectors Employed by Radar Sensor Systems

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Abstract: This paper is devoted to detection performance evaluation of the constant false alarm rate (CFAR) detectors employed by radar sensor systems used to construct the middle range radar (MRR) and short range radar (SRR) based on linear frequency modulation continuous wave (LFMCW) radar sensor system. Several CFAR detectors are compared under the same initial conditions and the evaluation criterion is an ability to detect the target return signals at different signal-to-noise ratio (SNR) with and without interfering targets. Simulation results are presented.

Keywords: Signal detection, Radar sensor, Constant false alarm rate (CFAR), Frequency modulation continuous wave (FMCW) radar sensor.

1. INTRODUCTION

Radar sensor system offers high information content and provide very good ranging ability and relative velocity measurement at the same time in addition to other advantages, namely, functioning under any weather conditions and harsh environments (dust, dirt, light, snow) [1]. The linear frequency modulation continuous wave (LFMCW) radar sensor system with 24 GHz operation frequency is a trend technology recommended for middle range radar (MRR) and short range radar (SRR) applications [2], for example, intelligent transportation and safety driving systems like blind spot detection (BSD) [3], and closing vehicle detection (CVD) [4].

In this paper, several constant false alarm rate (CFAR) detectors are discussed, namely, the cell averaging CFAR (CA-CFAR) detector, the ordered statistic CFAR (OS-CFAR) detector, the generalized censored mean level (GCML) detector, and the adaptive censored greatest-of CFAR (ACGO-CFAR) detector. All these detectors can be employed by LFMCW radar sensor system and are compared by target return signal detection performance under the same initial conditions. We consider two main cases. The first case if there are no any interfering targets. The second case when there are one or more interfering targets. The performance analysis for the proposed detectors is made based on simulation.

The paper remainder is arranged as following: the LFMCW radar sensor waveforms and relation between the beat frequencies, the target range and relative velocity are presented in section 2. The CFAR detectors are analyzed in section 3. In section 4, the performance comparison and the simulation results are introduced. Finally, the conclusions are discussed in section 5.

2. LFMCW RADAR SENSOR WAVEFORMS

The LFMCW radar sensor system changes the transmitted waveform frequency linearly as a function of time. The modulating waveform consists of two

sweeps: the up-sweep and down-sweep (triangle waveform). This shape helps us to define the target range and relative velocity between the radar sensor and target [5]. The instantaneous transmitted frequency $f_T(t)$ can be presented in the following form:

$$f_T(t) = \begin{cases} f_c + \frac{B}{0.5T_m}t, & 0 < t < 0.5T_m \\ f_c - \frac{B}{0.5T_m}t, & 0.5T_m < t < T_m, \end{cases} \quad (1)$$

where f_c is the radar sensor operation frequency, B is the transmitted waveform bandwidth (sweep bandwidth), and T_m is the sweep time. The sinusoidal LFMCW transmitted signal $S_T(t)$ is defined as:

$$S_T(t) = \sin \left[2\pi \left(f_c t + \frac{B}{T_m} t^2 \right) \right]. \quad (2)$$

The target return signal delay in the case of moving target (with Doppler shift) takes one of the following forms:

$$\tau = \begin{cases} \frac{2(R - V_r t)}{c} & \text{for approaching target;} \\ \frac{2(R + V_r t)}{c} & \text{for receding target,} \end{cases} \quad (3)$$

where R is the target range, V_r is the relative velocity between the radar sensor system and the target, and c is the speed of light. The target return signal coming in at the input of the detector is defined in the following form:

$$S_R(t) = \sin \left\{ 2\pi \left[f_c (t - \tau) + \frac{B}{T_m} (t - \tau)^2 \right] \right\}. \quad (4)$$

The difference in frequency between the transmitted and target return signals is called the beat frequency that is very important to define the target parameters. The frequency difference during the up-sweep part of the modulating waveform is the up-beat frequency f_{bu} , and the frequency difference during the down-sweep part of

the modulating waveform is the down-beat frequency f_{bd} . The relation between these beat frequencies and the target parameters R and V_r is illustrated by the following equations:

$$f_{bu} = \frac{4BR}{T_m c} - \frac{2V_r}{c} f_c, \quad f_{bd} = \frac{4BR}{T_m c} + \frac{2V_r}{c} f_c. \quad (5)$$

In practice, the target return signal is corrupted by noise and interference. Thus, the signal detection is a complicated problem and detection performance is an important factor for evaluation of any radar sensor system. By these reasons, the CFAR detector is an attractive solution for signal detection in radar sensor system.

3. CFAR Detectors

For any radar sensor system with high duty cycle, for example, FMCW radar sensor, the noise sensitivity seems to be very serious and important problem. Constant probability of false alarm P_{FA} is a desirable requirement for most radar sensors applications. Thus, there is a need to define the target return signal detection threshold based on the noise power (or noise variance) estimation that is varied as a function of time. The CFAR technique is based on implementation of the Neyman-Pearson criterion that can be expressed more formally for signal detection terminology as follows: there is a need to fix the probability of false alarm P_{FA} and maximize the probability of detection P_D . In any CFAR detector, the noise power is estimated after processing the number of reference cells using the sliding window technique. The required threshold is defined by multiplying the estimated noise power with scaling factor. This threshold is compared with signal power in the test cell or cells (the cell that is under investigation). The CFAR detectors are differed based on reference cells processing method and scaling factor. The threshold of any CFAR detector can be presented in the following form [6]:

$$V_T = TZ, \quad (6)$$

where T is the scaling factor, and Z is the estimated noise power. The relation between the P_{FA} , threshold, and the noise variance can be defined as:

$$P_{FA} = \exp\left(-\frac{V_T^2}{2\sigma_n^2}\right), \quad (7)$$

where σ_n^2 is the noise variance. We consider four types of CFAR detectors.

3.1 CA-CFAR detector

The CA-CFAR detector [6] has an optimum performance under homogeneous noise conditions when the neighboring reference cells contain the noise samples with the same statistics as the test cell. This detector is relatively simple. It estimates the noise power by averaging the power values of the data samples in the reference cells of the sliding window and then defines the threshold. A basic CA-CFAR detector

structure is shown in Fig. 2.

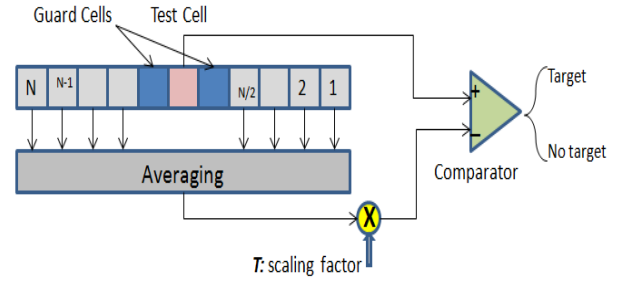


Fig. 1 CA-CFAR detector main structure.

The estimated noise power is given in the following from:

$$Z_{CA} = \frac{1}{N} \sum_{i=1}^N X_i, \quad (8)$$

where X_i , $i=1, \dots, N$, are the square law detector output samples (that are stored by the reference cells) where the output signal amplitude is proportional to the square of the input signal amplitude. The probability of detection P_D can be presented in the following form:

$$P_D = \left[1 + T(1 + \overline{SNR})\right]^{-N}, \quad (9)$$

where \overline{SNR} is the average signal-to-noise ratio. The scaling factor for CA-CFAR detector is a function of the number of cells N and the P_{FA} :

$$T = (P_{FA})^{-1/N} - 1. \quad (10)$$

3.2 Ordered statistic OS-CFAR detector

In many practical cases, the non-homogeneous noise conditions can be happened according to spatial and temporal variations in the noise power or closely spaced target return signals that may cause a bias in the estimated noise power and, consequently, the threshold. The OS-CFAR detector is designed to work under non-homogeneous conditions [7]. In the multi-target case, the performance of OS-CFAR detector is much better than mean level CFAR detectors family that includes the CA-CFAR, greatest of CFAR (GO-CFAR), and smallest of CFAR (SO-CFAR). This detector rearranges the reference cells data samples $\{X_1, \dots, X_N\}$ to form a new sequence according to the increasing power $\{X_{(1)} \leq X_{(2)} \leq \dots \leq X_{(k)} \leq \dots \leq X_{(N)}\}$, where the $X_{(k)}$ element of the ordered samples is called the k th order statistic which is selected as a representative of the noise power (Fig. 3). This approach is based on the fact that the interfering target signal power is usually higher than the noise power. Thus, the OS-CFAR is able to reject the number of interfering targets equal to $N-k$ located in the reference window. The minimal loss for this detector is achieved when the k has a reasonable value given by

$$k = \frac{3}{4} N. \quad (11)$$

The probability of detection P_D for OS-CFAR is

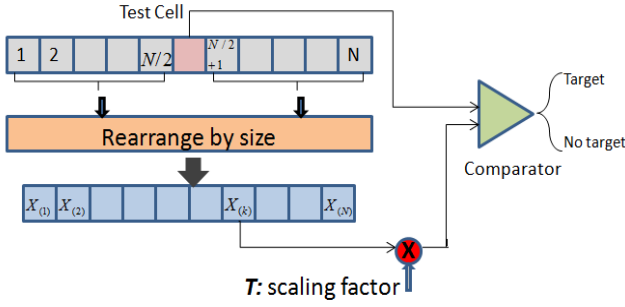


Fig. 2 OS-CFAR detector main structure.

determined by the following from:

$$P_D = \prod_{i=0}^{k-1} \frac{N-i}{N-i + \frac{T}{1+SNR}} \quad (12)$$

The scaling factor in this case is given by

$$T = (P_{FA})^{-1/k} - 1.$$

Finally, the threshold is determined as:

$$V_T = TZ = TX_{(k)}. \quad (13)$$

3.3 GCML detector

This detector operates under the non-homogeneous noise conditions [8]. The GCML detector defines the number and location of interfering targets in the reference window and discards them prior to define the noise power and the threshold, so there is no need to know the number of interfering targets (Fig. 4).

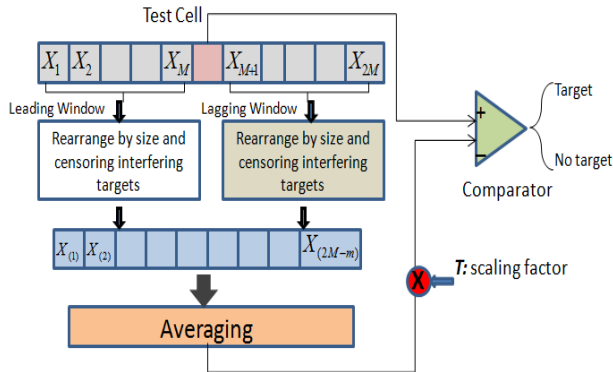


Fig. 3 GCMLD main structure.

The reference window is divided into two windows equal by length, the leading window $\{X_1, X_2, \dots, X_M\}$ when $M = N/2$, and the lagging window $\{X_{M+1}, X_{M+2}, \dots, X_{2M}\}$. These two windows are processed independently and in parallel way by the censoring processors. The censoring algorithm ranks the outputs of these two windows in ascending order of the amplitude like $\{X_{(1)} \leq X_{(2)} \leq \dots \leq X_{(M)}\}$ and $\{X_{(M+1)} \leq X_{(M+2)} \leq \dots \leq X_{(2M)}\}$ respectively. The algorithm considers the lowest order $X_{(1)}$ as the noise power representative and defines the threshold $V_{X(1)} = T_1 X_{(1)}$. This threshold is compared with $X_{(2)}$ and if $X_{(2)}$ is greater than $V_{X(1)}$ the censoring processor decides that the data samples corresponding

to $\{X_2, X_3, \dots, X_M\}$ are signals from interfering targets, and if $X_{(2)} < V_{X(1)}$ the algorithm decides that $X_{(2)}$ is a noise sample without interference. After that the censoring algorithm forms the sum of two lower ordered samples $X_{(1,2)} = X_{(1)} + X_{(2)}$ and defines the threshold $V_{X(1,2)}$ and compares this threshold with $X_{(3)}$. The censoring process is stopped when the hypothesis H_1 is decided to be true. More details about this detector can be found in [8].

3.4 ACGO-CFAR detector

This detector can be considered as a modified version of the GCML detector in order to reduce the clutter edge false alarm, when the test cell is at or near the boundary between two interference regions. Thus, the statistics in the leading and lagging windows will not be the same [9]. The detector suppresses the clutter edge false alarm by calculating the average noise power in the leading and lagging windows separately after applying the censoring process, and then selects the highest averaged value to consider it as the required estimated noise power. The structure of this detector is shown in Fig. 5.

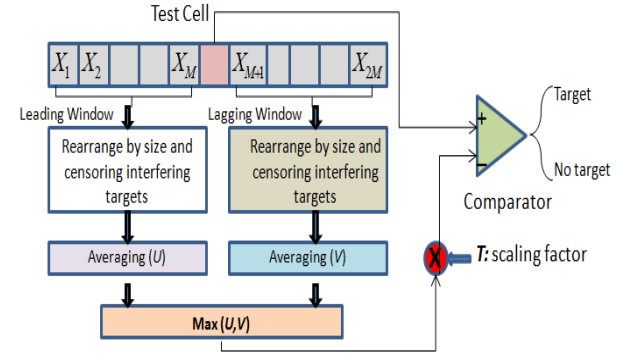


Fig. 4 ACGO-CFAR detector main structure.

Assuming that after applying the censoring process to the leading and lagging windows, n_1 samples are censored from the leading window cells and are censored from the lagging window cells, the remaining samples from the leading window $m_1 = M - n_1$ and from the lagging window $m_2 = M - n_2$ are used to estimate the noise power as follows:

$$U = \frac{1}{m_1} \sum_{i=1}^{m_1} X_{(i)}, \quad V = \frac{1}{m_2} \sum_{i=1}^{m_2} X_{(i)}. \quad (14)$$

The estimated noise power is set to be the maximum of U and V :

$$\hat{\sigma}_n^2 = \max(U, V). \quad (15)$$

4. SIMULATION RESULTS

The detection performances of all the discussed detectors are compared in terms of the probability of detection P_D for a specific range of SNR. The P_D is defined as the ratio between the number of observed components that exceed the threshold K and the total

number of observations M :

$$P_D = \frac{K}{M}. \quad (16)$$

The performance evaluation is made in two cases. The first case- there are no interfering targets, and the second case- an existence of interfering targets is taken into account. All detectors are evaluated under the same initial conditions. Table. 1 shows the main simulation parameters.

Table. 1 Main simulation parameters.

Simulation Conditions	
Carrier frequency	24 GHz
Bandwidth (B)	600 MHz
Modulation time (T_m)	0.0625 s
First target range (R_1)	60 m
First target relative velocity (V_{r1})	10 m/s
Second target range (R_2)	63 m
Second target relative velocity (V_{r2})	10 m/s
P_{FA}	10^{-4}
Reference cell (N)	20
Selected cell (K th)	15 th (for OS)
Signal power	100 mW
Number of observations (M)	1000
$R_3 = 66$ m, $R_4 = 70$ m, $R_5 = 73$ m, $R_6 = 76$ m	
$V_{r3} = V_{r4} = V_{r5} = V_{r6} = 10$ m/s	
Subject target is modeled as Swerling 2	
Interfering targets are modeled as Swerling 2	

Figure 5 shows a comparison between CA and OS-CFAR detection performance when there are no interfering targets, and when there are one and two interfering targets. If there are no interfering targets, the CA-CFAR detector performance is better, but if one or two interfering targets are presented, the OS-CFAR performance is much better and the CA-CFAR performance is very low.

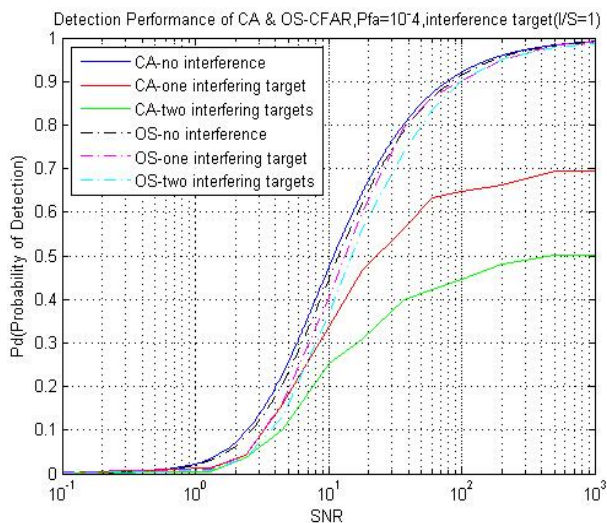


Fig. 5 CA & OS-CFAR performances comparison.

Figure 6 demonstrates a comparison between three detectors, namely, OS-CFAR, GCML, and ACGO-CFAR when there is no interference. The curves

are very close with slightly vantage to GCMLD.

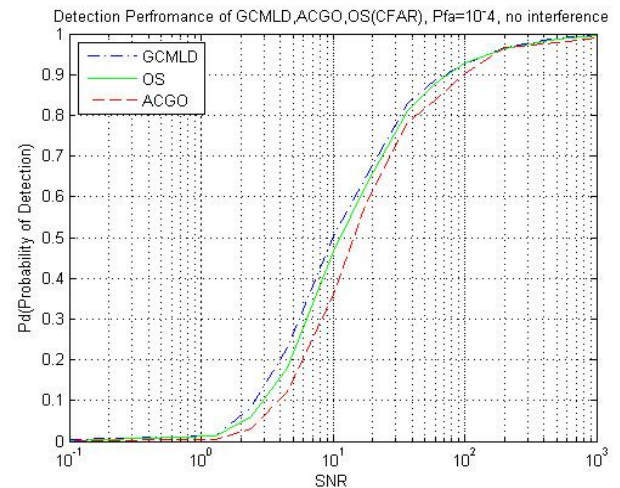


Fig. 6 Performance comparison (no interference).

Figures 7 (one interfering target) and 8 (two interfering targets) present robustness and the same performance ranking of OS-CFAR, GCML, and ACGO-CFAR detectors as in Fig. 6.

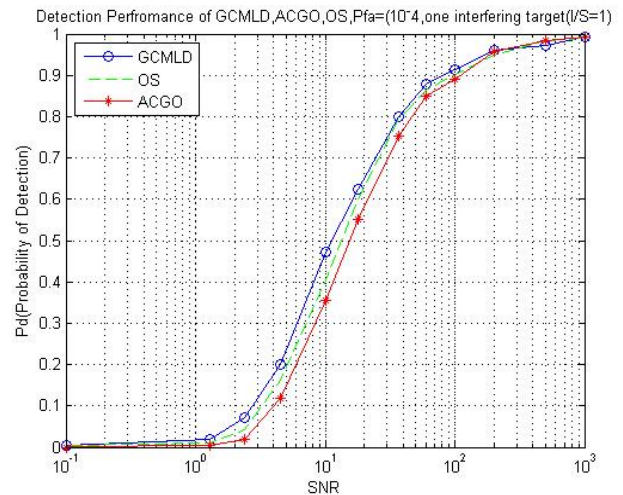


Fig. 7 One interfering target case.

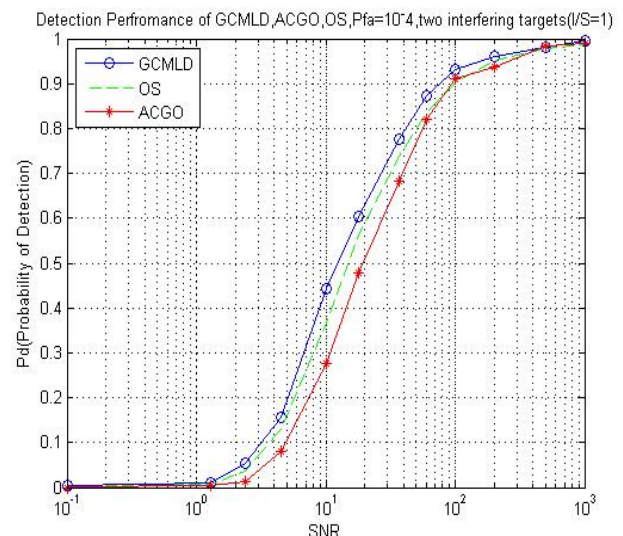


Fig. 8 Two interfering targets case.

Figure 9 presents the performance of OS-CFAR, GCML, and ACGO-CFAR detectors when there are five interfering targets. In this case, all detectors show considerable degradation in the performance and also keep similar ranking as before except that the CA-CFAR detector for high SNR values (more the 20 dB) has the lowest performance.

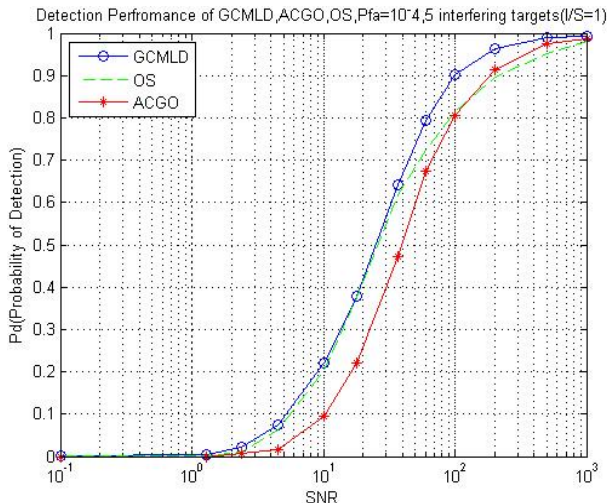


Fig.9 Comparison with 5 interfering targets.

Figure 10 demonstrates that the OS-CFAR performance is the worst. The reason is that there are six interfering targets, and the designed OS-CFAR can deal with no more than five interfering targets since $N = 20$ and the $k_{th} = 15$ ($N - k = 5$). Thus, to have five interfering targets is a critical case and one more interfering target causes big performance degradation.

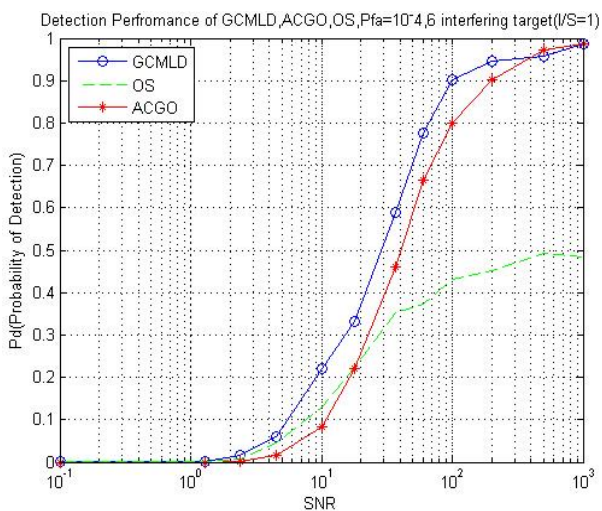


Fig. 10 Comparison with 6 interfering targets.

5. CONCLUSIONS

Based on the theoretical analysis, the simulation is carried out under conditions closed to practice to evaluate the presented CFAR detectors employed by FMCW radar sensor in the case when the interfering targets are absent and present. The CA-CFAR is the optimal detector among all other detectors under homogeneous noise conditions and when there are no

interfering targets (target masking). The OS-CFAR detector suffers from minor degradation in the detection performance in comparison with CA-CFAR detector, but its performance in multi-target situation is clearly superior to CA-CFAR for a specific number of interfering targets that is known priori. The GCMLD and ACGO-CFAR detectors maintain a strong robustness against the interfering targets regardless of the number of the interference signals in addition to that the ACGO-CFAR detector is capable to suppress the clutter edge false alarm. The GCMLD has the best overall detection performance in homogeneous and non-homogeneous noise conditions, but the main disadvantage of this detector is a very high computation cost as in the case of ACGO-CFAR detector. Thus, the OS-CFAR detector can be considered as the best trade-off between the detection performance and complexity.

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